A High Speed, Low-Cost Process for the Demodulation and Detection in EDGE

Wireless Cellular Systems

U.S. Patent Application of:

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TITLE OF INVENTION

A High Speed, Low-Cost Receiver for the Demodulation and Detection in EDGE
Wireless Cellular Systems

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CROSS-REFERENCE TO RELATED APPLICATIONS

Not applicable.

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STATEMENT REGARDING FEDERALLY SPONSORED RESEARCH OR DEVELOPMENT
Not Applicable

DESCRIPTION OF ATTACHED APPENDIX
Not Applicable

This invention relates to the demodulation and decoding of data transmitted for the so-called EDGE (Enhanced Data Rates for Global Evolution) system in the field of high-speed digital wireless communication.

5 **Background of the Invention**

An important factor limiting the wide application of wireless internet service is the slow data rate that current cellular system can support. As a high speed alternative, EDGE is one of the third-generation (3G) mobile wireless communication standards. The significance of EDGE is that it builds upon and improves the widely popular GSM

10 cellular system. Without altering the spectral characteristics of GSM, EDGE signal is required to provide high data service by upgrading the binary PSK (phase shift keying) signaling into an 8-PSK modulation. In EDGE systems, every three coded bits are Gray-mapped into an 8-PSK symbol, bring a single user data rate up to 384kbps. To allow EDGE signal to fit under the GSM spectrum mask, the modulated 8PSK symbols

15 are passed through a GMSK (Gaussian Minimum Shift Keying) pulse-shaping filter. This linearized GMSK pulse is the dominant component in the Laurent linear decomposition of GMSK signals [1].

Since the impulse response of the GMSK shaping filter spans primarily 5 symbol

20 periods, it introduces severe (known) partial-response ISI (inter-symbol interference) to the signals even for ideal channels. Given the 8-PSK modulation in EDGE, maximum likelihood sequence estimation (MLSE) based on the full-state trellis Viterbi algorithm becomes too complex for channels with long or even moderate ISI delay spread. Given

an ISI channel consisting of pulse-shaping filter and propagation distortion, the total

channel length spans N (> 5) symbol durations. The resulting number of states in a full-

state trellis equals 8 to the power of N-1. For a Typical Urban (TU) environment [2], the

total channel length N could be as large as 6, thereby requiring a total of 32768 states,

5   which is too costly to be implemented to hardware upon current technology. To alleviate

the computational complexity, reduced-state suboptimal MLSE equalizer using delayed

decision feedback (DDF) sequence estimation [3] has been adopted to EDGE

equalization preceded by channel re-shaping prefilters. Typically, significant

performance loss accompanies these suboptimal MLSE schemes.

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To further improve the detection performance, the procedure of turbo

equalization can be explored. Turbo detection for EDGE system may be applied with a

full-state Max-Log-MAP channel equalizer [4]. To simplify the highly complex Max-Log-

MAP equalizer, a simpler MMSE-BDFE with *a priori* information can be utilized [5]. To

15   achieve a good tradeoff between the detection performance and the computational

complexity, a suboptimal MAP equalizer *combining* soft output Viterbi algorithm (SOVA)

[6] and reduced-state trellis formed by DDF can be very effective [7]. It is important to

note, however, that this DDF-SOVA is still subject to error propagation. In fact,

decision feedback error propagation is a major factor that degrades the equalizer output

20   reliability.

The objective of the present invention is to improve the EDGE receiver by

alleviate error propagation by integrating the bi-directional arbitrated decision in EDGE

detection. Bi-directional processing was originally designed to improve the symbol

detection accuracy for decision feedback equalizer (DFE) by making arbitrations between the output sequences from two DFEs operating on opposite directions. For suboptimal EDGE turbo equalization system, soft decisions are needed. Hence, we add a reversed-time DDF-SOVA equalizer, which processes the time-reversed signal

5 sequence of the received EDGE signal bursts, to the existing forward DDF-SOVA equalizer. The soft outputs from the forward and reverse DDF-SOVA equalizers are integrated to exploit the time-reversal diversity resulted from the error propagation in DDF reduced-state trellis processing. A simple scheme for combining soft-information from the forward and reverse DDF-SOVA equalizers is also invented.

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Due to the use of channel re-shaping prefilters as feedforward filter to reduce feedback DDF trellis, a much low complexity DDF-SOVA equalizer can be practically implemented. By applying the bi-directional arbitrated decision DDF-SOVA architecture into EDGE detection, a much reliable and low complex EDGE detection scheme

15 become practical.

Summary of the Invention

The primary aspect of the invention is to present a low cost, practical receiver technology that meets and improves the detection performance of EDGE system

20 providing a signal received from a single antenna, comprising the steps of: for every 4 bursts of received signal corresponding to the transmitted EDGE frame of 592 symbols, sampling at the symbol rate; and storing the sampled data to estimate the wireless channel impulse response via cross-correlation according to the mid-amble training data in all 4 bursts; and designing MMSE pre-filter and DFE (decision feedback equalizer)

based on the channel estimates [8]; and reversing the channel response to design a time-reversed (TR) MMSE pre-filter and a DFE; and processing all the received data samples once by the first (forward time) pre-filter and DFE; and processing the TR signal samples by the second (time-reversed) pre-filter and DFE; and taking both soft

5 outputs from the two DFE output to form a weighted combination for soft-output 8PSK symbol value from the equalizer; and deriving soft-bit outputs from the soft 8PSK symbol output value via Max-Log nonlinearity; and de-interleaving the bit soft-outputs before sending them to a MAP decoder for the FEC (forward error correction) code; and generating soft extrinsic [6] output from the MAP decoder; and interleaving MAP outputs

10 before forming the soft bit extrinsic information; and feeding the soft bit extrinsic information directly to DFE to complete the iteration; and terminating the said turbo-equalization when extrinsic information become stable.

The step of signal collection and channel estimation comprises sampling 4 bursts

15 of modulated signals based on an acquired timing clock, storing the received data samples in memory, using cross-correlation between the training mid-amble and the received data to estimate the nearly-stationary, unknown wireless channel response.

The step of pre-filter and DFE design can comprise the MMSE (minimum mean

20 square error) design in the forward direction, and the MMSE filter design based on the received channel response and reversed data sample sequence.

A key element for simplifying the receiver complexity requires the use of a bi-directional equalizer, comprising: a forward direction DFE with pre-filtering and a

reverse direction DFE with pre-filtering; a max-log nonlinearity in the forward and the

reverse equalizers to generate soft bit value information; a hard decision device for

generating decision bits that form the DFE filter input in the forward and the reverse

direction; a summation prior to the hard-decision device for inputting soft extrinsic

5   values; and a weighted linear combiner to combine the forward DFE and the reverse

DFE soft-symbol information to be sent to the de-interleaver and the MAP decoder.

Another aspect of the invention provides a generalization of the bi-directional

DFE through the use decision-delayed feedback (DDF) for improved performance using

10   reduced state trellis, comprising: a soft-output-Viterbi-algorithm (SOVA) equalizer that

directly provides soft bit information for turbo processing; a flexible design of trellis with

different levels of complexity according to the number of states 8^{k-1} determined by the k

leading samples of the channel impulse response.

15   Each receiver can comprise more than one antenna and radio frequency circuits

for providing multiple received signal sequences corresponding to the same transmitted

data frame, and can be directly incorporated in the bi-directional equalizer design with

the estimation of a single-input-multiple output channel response and the design of

multiple-input-single-output pre-filters in both the forward and the reverse directional

20   circuits.

Each receiver can also comprise faster samplers for providing multiple received

signal sequences corresponding to the same transmitted data frame, and can be

directly incorporated in the bi-directional equalizer design with the estimation of a single-

input-multiple output channel response and the design of multiple-input-single-output pre-filters in both the forward and the reverse directional circuits.

Other objects and advantages of the present invention will become apparent from the following descriptions, taken in connection with the accompanying drawings, wherein, by way of illustration and example, an embodiment of the present invention is disclosed.

Brief Description of the Drawings

The drawings constitute a part of this specification and include exemplary

5   embodiments to the invention, which may be embodied in various forms. It is to be

understood that in some instances various aspects of the invention may be shown

exaggerated or enlarged to facilitate an understanding of the invention.

Figure 1 is the block diagram of DDF-SOVA turbo receiver for EDGE wireless

10   communications system.

Figure 2 is the block diagram of a transmitter in communications system.

Figure 3 is the block diagram of a conventional receiver in communications

system.

Figure 4 is the modulation procedure of EDGE's 8-PSK signal.

15   Figure 5 is the constellation for 8-PSK Gray mapping in EDGE system.

Figure 6 is the linearized GMSK shaping pulse in EDGE system.

Figure 7 is the format of an EDGE burst.

Figure 8 (a) is the magnitude of a symbol-rate sampled TU channel impulse

response. Figure 8 (b) is the magnitude of the channel impulse response after

20   prefiltering.

Figure 9 is the bock diagram of bi-directional DDF-SOVA turbo receiver for

EDGE wireless communications system.

Detailed Description of the Preferred Embodiments

Detailed descriptions of the preferred embodiment are provided herein. It is to be understood, however, that the present invention may be embodied in various forms.

5   Therefore, specific details disclosed herein are not to be interpreted as limiting, but rather as a basis for the claims and as a representative basis for teaching one skilled in the art to employ the present invention in virtually any appropriately detailed system, structure or manner.

10   Referring to Fig. 2, there is shown the basic block diagram of a baseband transmitter in a communications system. The input information bits first go into a channel encoder to introduce redundancy for the purpose of error correction at the receiver side. Then the coded bits are sent into the modulator to form the transmitted symbols according to the specific modulation rules such as QAM, PSK and so on.

15   Those modulated symbols finally are transmitted into the non-perfect channel with intersymbol interference.

Referring to Fig. 3 shows the structure of a digital baseband processing portion of a conventional receiver in a communications system. The received signal samples

20   are first passed into the channel equalizer to compensate the channel intersymbol interference. The estimated symbols are then sent to the demodulator to generate bits according to the specific modulation rules. Afterward, the channel decoder recovers the information bits from the output of demodulator.

Referring to Fig. 4 illustrates the specific modulation procedure in an EDGE

transmitter. Every three encoded bits are converted into an 8-PSK symbol based on

Gray mapping. The constellation of Gray mapping is shown in Fig. 5. To avoid signal

envelope zero-crossing, the modulated symbols are continuously rotated by $3\pi/8$ on a

5   symbol-by-symbol basis. To make EDGE signal fit into GSM spectrum mask, the

rotated symbols are sent into a linearized GMSK pulse-shaping filter. As shown in Fig.

6, the duration of this filter impulse response last about 5 symbols. As a result,

significant intersymbol interference is introduced even before the signal is sent into the

channel.

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Referring to Fig. 1, there is shown the block diagram of the EDGE turbo

receiver. Unlike the conventional receiver structure as shown in Fig.3, the turbo receiver

has information feedback path from **18, 19, 20, 21** to **15**. The turbo receiver consists of

seven components, namely, channel estimator **22**, prefilter **14**, soft-input-soft-output

15   channel equalizer **15**, deinterleaver **17**, soft-input-soft-output channel decoder **18**,

detection controller **19** and interleaver **20**. Specifically in this embodiment, a DDF-

SOVA equalizer is used as the soft-input-soft-output equalizer **15** for its low

implementation complexity. The soft-input-soft-output decoder **18** could be any MAP or

suboptimal MAP decoder.

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Channel estimator **22** is used to estimate channel impulse response and provide

coefficients to the prefilter **14** and channel equalizer **15**. The channel could be estimated

by using the training sequence, which is available in each EDGE burst as shown in Fig.

7.

After first turbo iteration, the estimated symbols of the whole burst could be used as training symbols to refine the channel estimate iteratively.

Prefilter **14** is designed to shorten the channel impulse response, which is critical to ensure good detection performance of the subsequent DDF-SOVA equalizer **15**. One embodiment of this prefilter **14** is to use the feedforward filter in a decision feedback equalizer (DFE) designed for the estimated channel. Subsequently, feedback filter coefficients of the DFE can be used by the DDF-SOVA equalizer **15** to form the corresponding trellis. Fig 8 (a) shows the magnitude of a TU channel impulse response. Fig 8 (b) shows the shortened channel impulse response with the assistance of a prefilter **14**.

Reduced-complexity soft-input-soft-output equalizer **15** is a critical component for the EDGE turbo receiver. In this embodiment, delayed decision feedback (DDF) sequence estimation approach is adopted to reduce the trellis state. In full-state trellis algorithm, trellis is formed based on all N channel taps. While in DDF, only the leading K < N channel taps are used to define the trellis, therefore the number of states is reduced from 8^{N-1} to 8^{K-1} for EDGE's 8-PSK modulation. Metrics are calculated based on symbols corresponding to current states as well as previously estimated symbols associated with the current survivor. Since only the first K channel taps are involved with the trellis structure, DDF operates well for channels with concentrated energy in the leading taps. This prompts the use of the prefilter **14** to re-shape the channel response. Based on the reduced-state trellis, any MAP algorithms can be chosen to calculate the soft output values, which is defined as:

$$L(c_k) = \log[\frac{\Pr(c_k = 1)}{\Pr(c_k = 0)}],$$

For EDGE system with 8PSK modulation, a transform soft values d_k between 8PSK symbols $\{S_k\}$ and coded bits $\{C_k\}$ is required, as a result, soft output values are calculated as:

$$L_{d^{(m)}}(d_k) = \log[\frac{\Pr(d_k = d^{(m)})}{\Pr(d_k = d^{(0)})}]$$

$$= \log[\frac{\prod_{i=1}^{3} \Pr(c_{k,i} = d^{(m)}(i))}{\prod_{i=1}^{3} \Pr(c_{k,i} = d^{(0)}(i))}]$$

$$= \sum_{d^{(m)}(i)=1} L(c_{k,i})$$

where $d^{(m)}(i)$ is the ith bit of symbol $d^{(m)}$, $c_{k,I}$ is the ith bit of the kth symbol.

In this embodiment, the soft-output-viterbi-algorithm (SOVA) is used for its simplicity.

The soft outputs from the channel equalizer **15** are deinterleaved by **17** and forwarded to the channel decoder **18**. The soft decisions on the encoded bits are then fed back into the channel equalizer **15** after interleaved by **21**. These soft decisions are referred as *a prior* information for the transmitted signal. The *a prior* information can assist the channel equalizer **15** to obtain more reliable signal detection in the next iteration. The subtractors **16, 20** are used to retain only the extrinsic soft values, which represent the incremental information about current bits (symbols). After a number of iterations which is controlled by detection controller **19**, hard decisions on the information bits can be made by slicing the soft values of the information bits.

To further improve the detection performance, bi-directional processing can be applied to the DDF-SOVA turbo equalizer as shown in Fig. 9. The bi-directional turbo equalizer includes two turbo equalizers **31,36**. One is referred as forward turbo equalizer **31**, which processes the received signal burst. Another is referred as reverse turbo equalizer **36**, which processes the reversed version of the received signal burst. In the reverse turbo equalizer, the prefilter and DDF-SOVA trellis coefficients are based on the DFE decomposition of the reversed version of the channel estimate. The soft decisions from the reverse turbo equalizer **36** are reversed by **35** and then linearly combined with the soft decisions from the forward turbo equalizer **31**. The combination weights for the two output sequences could be simply equal. They can also be chosen based on other criterions.

APPLICATION AREAS OF THE PRESENT INVENTION

EDGE Handset Receiver Design;

EDGE Base Station Receiver Design;

Wireless LAN Receiver Design;

Wireless Mobile Communication Systems Design;

Personal Communication Systems Design;

Summarizing, according to the invention, a process for demodulation and detection in EDGE wireless cellular systems comprises an accurate estimator for wireless channel response, a memory block storing received data frame, a time-reversed block processor, a forward block processor, a soft-output Viterbi signal detector, a convex combinator of forward and reverse block processing outputs, a maximum a-posteriori (MAP) equalizer consists of forward and reverse soft-output Viterbi processing blocks, a de-interleaver prior to MAP decoding, a MAP decoder, and an interleaver for passing MAP decoder soft output to the MAP equalizer .